SWEEP METHOD USING DIGITAL SIGNALS

Field of the Invention

The invention relates to a method, system, and apparatus for providing a high resolution, non-intrusive determination of frequency response for a cable television (CATV) network carrying one or more digital channels.

Background of the Invention

Digital television signal broadcasting has several advantages over traditional analog television signal broadcasting. A digital data channel, as with an analog channel, is susceptible to noise, but so long as the received signal overcomes a threshold signal-to-noise level, the transmission is essentially error-free. Channel distortion and noise can be corrected in a digital system by using adaptive equalizers, as well as various error correction and error tolerance methods. Employing coding techniques overcomes channel-related signal impairments and optimizes bandwidth efficiency. Therefore, digital television signals are less susceptible to image distortion and interference. As a result, digital television signals require less bandwidth for comparable image and sound quality.

A typical digital cable television (CATV) system transforms an analog television (TV) signal into a linear pulse-code-modulation (PCM) digital representation of an image. Processing of the transmitted digital signals is done according to a particular application, the processing including frame synchronization and time-base correction, correction for luminance and chrominance error, image manipulation that allows digitally generated effects and graphics to be added to an image, and data compression.

Converting an analog signal to a digital signal is achieved by means of an analog-to-digital (A/D) converter. The A/D typically consists of four components: a band-limiting antialiasing filter, a sample-and-hold circuit that samples the analog signal, a

quantizing unit that divides the range of each analog signal sample into a number of distinct levels, and an encoder that places a specified code on the output data lines for each of the quantized levels.

A receiver of the digital signals typically includes a digital-to-analog (D/A) converter having a digital input register in which the bits of a received word are stored, a decoder for converting the data lines into the number of quantized distinct analog levels, a resampling circuit for correcting distortion error introduced by the sample-and-hold, and a band-limiting filter.

Although a digital communication system can be made essentially error-free, the transmission over a physical medium is still susceptible to misalignment, temperature-related drift, and induced noise and impedance variation. The variations due to the physical medium and the system's analog components can be analyzed using various tests. One such test is a sweep test.

A frequency sweep test involves performing measurements over a range of frequency values in order to obtain frequency response information. In order to frequency sweep test a communication system such as a CATV system, a conventional test setup may use a headend test unit connected to the CATV system at its headend and a remote test unit connected to the CATV system at a desired location. In a conventional test, the headend unit sends frequency sweep test signals over the network to a remote test unit. Telemetry signals are utilized to coordinate the operation of the remote test unit with the headend test unit. The headend test unit sequentially injects test signals at each channel frequency and the remote test unit measures signal strength for each respective frequency. The remote test unit determines the frequency response of the CATV system based the results of the sweep test.

A problem with the conventional frequency sweep test is that it disrupts service to the CATV subscribers because the injected test signal interferes with their reception of the corresponding channel. In order to correct this problem, a conventional sweep test

system uses a transmission scheme that has a controller which stores a list of channel frequencies to be swept, so that a test signal is generated and transmitted for a particular channel frequency only if a TV signal is not being transmitted on that channel, and the television signals themselves are used as test signals on those channels having a current TV transmission.

Such prior non-invasive sweep systems, however, are designed for use with analog CATV channels that carry television signals having the NTSC format. To this end, the prior sweep systems perform measurements based upon certain standard pulses within the analog television signal. For example, analog sweep tests often rely on vertical synchronization pulses in the performance of measurements because they are predictable in both magnitude and occurrence. Such analog sweep systems are not applicable to digital television signals, which do not include such pulses (e.g., sync pulses). Moreover, such prior art systems often provide limited resolution, typically a single measurement per channel.

A method and apparatus for sweep testing a *digital* broadband television signal has been defined by U.S. Patent 6,061,393, issued to Tsui, et al.. However, the method therein described only computes an estimate of a system response that is then deconvolved to isolate particular components. In addition, that method requires that an impulse be fed into the system and, thus, can be invasive.

Accordingly, there is a need for a sweep measurement method that is non-invasive and can be used on digital communication channels. There is a further need for such a system that has improved resolution over prior art non-invasive systems.

Summary of the Invention

The present invention satisfies the above-stated need, as well as others, by providing a method of determining a frequency response of a channel by obtaining a relative frequency response of the channel and an overall channel signal strength. The

present method combines these obtained values to generate an absolute level frequency response. The use of an absolute level frequency response allows the frequency response for the measured channel to be combined with frequency response information from other channels, digital or analog, to obtain a system frequency response of high resolution and which may be accomplished in a non-invasive manner.

A method of determining a frequency response of a communication system includes tuning to a selected digital channel frequency, obtaining an absolute signal strength measurement for the selected digital channel frequency, obtaining relative frequency response measurements for the particular selected digital channel, and combining the relative frequency response measurements and the absolute signal strength to obtain an absolute level frequency response for the selected digital channel.

An apparatus for determining a frequency response of a communication system includes a tuner operative to tune to a selected digital channel frequency band, and a measurement circuit. The measurement circuit is operative to obtain absolute signal strength measurements for the selected digital channel frequency band, and obtain relative frequency response measurements for the selected digital channel frequency band. The measurement circuit is further operative to combine the relative frequency response measurements and the absolute signal strength measurements to obtain an absolute level frequency response for the selected digital channel frequency band.

The above described embodiments provide a channel response on an absolute scale that has relatively high resolution. Because the response is on an absolute scales, the channel response may be combined with other absolute channel responses to obtain a system response of relatively high resolution. Optionally response for frequencies between channels may be interpolated.

The above-described features and advantages, as well as others, will become more readily apparent to those of ordinary skill in the art by reference to the following detailed description and accompanying drawings.

Brief Description of the Drawing

FIG. 1 is a block diagram illustrating an exemplary communication system for transmission of broadband signals and testing a frequency response of the system.

FIG. 2 is a simplified block diagram illustrating a testing unit for sweep testing according to an embodiment of the invention.

FIG. 3 is a simplified representation of a mixer and lowpass filter used to convert a tuner output to a baseband signal according to an embodiment of the invention.

FIG. 4 illustrates an output of the sweep tester having frequency response information for four channels.

FIG. 5 is a depiction of an ideal QAM-64 constellation.

FIG. 6 is a flowchart showing an exemplary method for determining the frequency response of a communications system according to the present invention.

Detailed Description

FIG. 1 shows a frequency response measurement device **10** according to the present invention implemented within a communication system **12**. The communication system **12** comprises a CATV distribution system and includes a headend transmission system **14**, a distribution network **16**, and a plurality of splitters **18** disposed along the distribution network **16**. It will be noted that the communication system **12** is shown in greatly simplified form, although it is representative of the general configuration of all terrestrial CATV distribution systems.

The frequency response measurement device **10** includes a tuning circuit **22** connected to the distribution network **16** via one of the splitters **18**, a measurement circuit **24** connected to the output of the tuning circuit **22**, and in the preferred embodiment described herein, a display **26** for displaying the results output by the measurement circuit **24**. The tuning circuit **22** is operable to tune to any of a plurality of digital channels, and

may suitably have a structure similar to that of an ordinary digital television receiver. The tuning circuit **22** receives a broadband television signal and generates a single digital channel signal therefrom.

The measurement circuit **24** is a circuit that is operable to receive a digital channel signal and generate an absolute level frequency response for the digital channel signal. To this end, the measurement circuit **24** is operable to obtain an absolute signal strength measurement for the entire digital channel frequency band. The measurement circuit **24** is further operable to obtain a relative frequency response measurement for the digital channel frequency band. The measurement circuit **24** is then operative to combine the absolute signal strength measurement with the relative frequency response to generate an absolute level frequency response for the digital channel frequency band. The measurement circuit **24** is also preferably operative to cause the tuning circuit **22** to tune automatically to one or more subsequent digital channel signals and obtain absolute level frequency responses for the subsequent digital channels. The measurement circuit **24** is preferably also operative to intepolate an absolute level frequency response between a maximum value of the absolute level frequency response of one channel and a minimum level of the absolute level frequency response of the other channel. In this manner, the absolute level frequency responses from several channels may combined to obtain a system frequency response having a relatively good resolution.

In the general operation of the communication system **12**, the headend transmission system **14** transmits a broadband signal that includes a plurality of digital channels onto the distribution network. The digital channels constitute carrier frequencies modulated using digital modulation techniques such as QPSK or QAM, techniques widely known in the art. Each digital channel occupies a defined digital channel frequency band within the broadband signal. The broadband signal propagates from the distribution network **16** to each of a plurality of subscriber systems **20**. The

subscriber systems **20** include one or more television receivers (not shown) that selectively receive one of the channels of the transmitted broadband signal.

From time to time it is advisable to obtain the frequency response of the communication system at one or more channel frequencies including those in which a digitally modulated signal is normally transmitted. To this end, the measurement device **10** is coupled to the distribution network **16** to obtain measurements therefrom. In particular, the tuning circuit **22** may be coupled to the distribution network **16** via a coupler **28**.

The tuning circuit **22** then tunes to a select digital channel and provides the select digital channel to the measurement circuit **24** as an intermediate frequency ("IF") channel signal. The measurement circuit **24** first obtains an overall signal strength measurement for the channel. The measurement circuit **24** further obtains a relative frequency response of the IF digital channel signal. The relative frequency response of a digital channel may typically be derived from the tap weights or coefficients of an adaptive equalizer or filter within the receiving circuitry. The resulting frequency response has relatively high resolution.

Further detail regarding an exemplary technique for obtaining a digital channel signal strength measurement and a relative frequency response measurement is provided below in connection with **FIGS. 2 to 6**. The measurement circuit **24** then combines the overall signal strength measurements with the relative frequency response to obtain an absolute level frequency response for the digital channel. The tuning circuit then tunes to a subsequent digital channel. The measurement circuit **24** obtains an absolute level frequency response for the subsequent digital channel using the techniques described above. The tuning circuit **22** may then tune to additional channels and the measurement circuit **24** may obtain absolute level frequency responses for such additional channels. The accumulated absolute level frequency responses may then be stored and/or displayed. However, there is often a gap between the highest frequency of one channel and the

minimum frequency of the next adjacent channel. To address this gap, the measurement circuit **24** preferably intepolates between the highest (maximum) frequency of one digital channel's absolute frequency response and the lowest (minimum) frequency of the next channel's response. The combination of the measured and intepolated response provides a continuous response over at least a multichannel portion of the bandwidth of the overall system.

In accordance with the present invention, the measurement circuit **24** combines the absolute signal strength with the relative frequency response of the channel to obtain an absolute level frequency response of the selected digital channel.

The absolute level frequency response is useful for a number of test purposes. For example, the measurement device **10** may be employed to obtain absolute frequency response for several channels which may be combined to provide a wideband frequency response. If only the *relative* signal levels were used, such a wideband frequency response would provide the frequency responses of the various channels without proper context.

The absolute level frequency response may also be combined with the frequency sweep results of ordinary analog channel responses to obtain a wide band frequency response. To this end, the absolute level frequency response may be combined with results from a conventional non-invasive analog sweep tester to provide an overall system response for a system that includes analog and digital channels. Alternatively, the measurement device **10** may itself be modified to also perform analog sweep testing. To this end, the measurement circuit **24** may be modified to include analog television measurement functionality such as that described in U.S. Patent 5,585,842, which is incorporated herein by reference.

The absolute level frequency response generated by the measurement circuit **24** of the present invention is also useful in determining the frequency response of one or more portions of the distribution network **16**. In particular, the degradation of the measured

frequency band can be determined by comparing the absolute level frequency responses from different locations in the distribution network **16**.

One reason the measurement circuit **24** of the exemplary embodiment of the present invention obtains a relative frequency response separate from the absolute signal strength is that a significant amount of frequency response information of a digital QAM or QPSK signal may be obtained through the partial or complete demodulation process, as taught by U.S. Patent No. 6,061,393 issued to Tsui et al. However, information obtained through digital signal demodulation omits the overall received signal strength, and thus only provides relative frequency response information.

FIG. 2 shows an exemplary embodiment of the measurement device **10** of **FIG. 1**. In **FIG. 2**, the tuning circuit **22** further comprises an attenuator **120** coupled to a tuner **140**. The measurement circuit **24** further comprises a processor **100**, a QAM demodulator **160**, and an I/Q decoder **180**. The measurement device **10** further comprises a keypad **110**.

The processor **100** may suitably be a microprocessor, microcontroller, or a combination of either or both devices with a digital signal processor (DSP) and/or discrete digital circuitry that performs processing functions as described herein. The processor **100** is preferably coupled to control the operation of the attenuator **120** and the tuner **140**. The processor **100** is operably coupled to cooperate with the QAM demodulator **160** to obtain relative frequency response measurements. The processor **100** is further coupled to the tuner **140** to receive raw signal strength information therefrom.

The exemplary QAM demodulator **160** shown in **FIG. 2** includes a sampler **150**, an adaptive equalizer **170**, and an I/Q decoder **180**. The sampler **150** receives the baseband signal from the tuner **140** and outputs digitized signals to the adaptive equalizer **170**. The I/Q decoder **180** is connected to receive the output signals from the adaptive equalizer **170** and generate equalizer update signals via an update mechanism **101**. The

equalizer update mechanism **101** outputs tap weight coefficients to the adaptive equalizer **170** in a feedback manner.

The sampler **150** is operative to digitize the tuner output signal to provide values I, Q that correspond to a QAM grid of signals, ideally shown by way of example in **FIG. 5**. The QAM signals I, Q from the sampler **150** are then adjusted by the action of the adaptive equalizer **170** in order to compensate, for example, for irregularities or variations in the distribution network **16**. The I/Q decoder **180** acts as a 'symbol decider' that equates a grid point to a signal within a range of the particular grid. Thus, an I/Q decoder **180** provides a source of error information by distinguishing an ideal point on, for example, a constellation such as that shown in **FIG. 5**, from the corresponding constellation point as produced by the adaptive equalizer **170**. This error information is provided to an update mechanism **101** as error signals E_x and E_y.

Although the QAM modulation scheme described herein employs a tuning/downconversion stage that develops two outputs, I and Q, that correspond to each orthogonal component, the present invention is not limited to any particular modulation scheme. Moreover, the QAM demodulator **160** as illustrated in **FIG. 2** is given by way of example only. The QAM demodulator **160** may readily be replaced with alternative configurations of a QAM demodulator that produce error signals from which new adaptive equalizer weights may be generated.

The EQ weight update mechanism **101** is a functional block that is operative to adjust the weights of the adaptive equalizer **170** based on error signals E_x and E_y received from the I/Q decoder **180**. The update mechanism **101** may be a part of the I/Q decoder **180** or the processor **100**, or may constitute a separate device or circuit. Update mechanisms that generate update equalizer weights are known. As will be discussed below, the updated equalizer weights are used by the adaptive equalizer to improve the receive digital signal as is known in the art, and are also used by the processor to generate the relative frequency response for the channel.

In operation, a keypad **110** inputs the desired test criteria to a processor **100**. An input broadband signal is fed to an attenuator **120** that actively changes its characteristics in order to obtain a maximum swing (dynamic range) within the associated sampler 150. The attenuated input signal then propagates to the tuner **140**, which provides the chosen band as an intermediate frequency signal to the demodulation 160.

The tuner **140** further provides raw signal strength information on signal line **141** to the processor 100. The raw signal strength information may suitably be instantaneous amplitude information such as that produced by a log amp detector or the like. The processor **100** converts the raw signal strength information into absolute signal strength measurements for the received digital channel. Such absolute signal strength measurements are also used to calibrate the tuner output based on a predetermined reference for each channel. The processor **100** may generate absolute signal strength measurements using any known technique for generating absolute signal strength measurements of a digital television signal, including those taught in U.S. Patent No. 6,041,076 to Franchville, et al., U.S. Patent Application Serial Number 09/259,508 to Chappell, or U.S. Patent Application No. 09/282,735 to Bowyer, all of which are incorporated herein by reference.

FIG. 3 shows in further detail an exemplary embodiment of the tuner **140** of FIG. 2. The tuner **140** employs IF bandwidth filters so that the IF signal has a 6 MHz bandwidth, as is well-known, e.g., Triad manufactures such a tuner for cable modems and settop boxes. The exemplary tuner **140** of includes a two stage mixing arrangement where a variable voltage-controlled oscillator (VCO) **145** generates a frequency for mixing with the incoming broadband signal in order to produce a predetermined first IF frequency at approximate 44.5 MHz. The 44.5 MHz. frequency is chosen for convenience and for the benefit of using commercially available component, such as the bandpass filter **149**.

The VCO **145** frequency is controlled by a control signal line from the processor **100**. The frequency of the VCO **145** is chosen such that the mixer **145a** will convert the desired channel frequency to 44.5 MHz. For example, if the selected channel has a center frequency of 100MHz, the processor **100** generates a voltage that causes VCO **145** to produce a frequency of 55.5 MHz, which is mixed with the 100 MHz broadband signal to produce the 44.5 MHz IF signal. The 44.5 MHz IF signal thus contains the desired channel. The bandpass filter **149** effectively filters out all but the 6 MHz bandwidth channel centered at 44.5 MHz.

The second stage of mixing converts the 44.5 MHz IF signal to baseband by mixing the frequency from local oscillator **143** with the IF signal (6 MHz bandwidth) using the mixer **148**. The lowpass filter **142**, combined with the mixer **148** and local oscillator **143**, produce a baseband IF signal having a center frequency of approximately 3 MHz and a bandwidth of 6 MHz, the low pass filter **142** assuring that the baseband IF signal has a sharp cutoff at the 6 MHz band. The tuner **140** baseband output signal propagates to the sampling circuit **150** of the QAM demodulator **160** (See **FIG. 2**).

The baseband IF signal may also propagate to a device such as a log amp detector **152**, which generates the raw signal strength information used by the processor **100** to determine absolute signal strength. The log amp detector **152** is operable to generate an analog signal having a DC voltage level that is representative of the magnitude of the input IF signal. The log amp detector 152 is operably coupled to provide the analog signal to an A/D converter **153**, which generates digital values representative of the raw signal strength. The A/D converter **153** then provides the digital values over line **141** to the processor **100**.

Referring again to **FIG. 2**, the quadrature amplitude modulation (QAM) demodulator **160** demodulates the tuner **140** baseband IF output. To this end, the demodulator **160** may suitably comprise a sampler **150**, an adaptive equalizer **170**, and an I/Q decoder **180**.

The sampler **150** converts the downconverted signal from the tuner **140** to a discrete-time digital representation of the raw in-phase (I) and quadrature (Q) components. The sampler **150** may be implemented by synchronizing the sampling rate to an external signal such as the input broadband signal or by directly using a sampling rate control signal. Such methods are known. Alternatively, an A/D converter (not shown) can be used to sample, for example, an input centered at an IF, a fixed sampling rate and IF being chosen in relation to the spectrum of the modulation signal so as to enable digital quadrature direct conversion to baseband by a digital QDC stage (not shown).

The adaptive equalizer **170** adjusts the I and Q values to correct for channel distortion. The adaptive equalizer **170** automatically corrects for distortions in the channel and typically includes a digital finite impulse response (FIR) filter and/or infinite impulse response (IIR) filter (not shown) with variable tap weights. In the exemplary embodiment described herein, the adaptive equalizer is an impulse response filter having various tap coefficients.

According to the invention, coefficients that correspond to adjustment of the tap weights are generated by the adaptive equalizer **170**. The adjustment time, when the tap weight coefficients are generated, is at or after the time the adaptive equalizer **170** acquires lock. In particular, as more I and Q samples are received, the adaptive equalizer 170 eventually achieves a relatively stable set of tap coefficients. At this time, the adaptive equalizer **170** is said to have "acquired lock".

The I/Q decoder **180** decodes the two orthogonal components, I and Q, and generates error signals E_x and E_y by comparing the ideal response characteristics to the data generated by the adaptive equalizer **170**. The I/Q decoder **180** examines the data output from adaptive equalizer **170** and estimates, or assigns, the I and Q values of the transmitted data based on rules that are specific to the modulation scheme being used. A

channel decoding scheme may also be used to remove effects of forward error correction or other channel coding schemes being applied to the data.

After the various coding schemes are accounted for, the decoder **180** generates the error signals E_x and E_y that correspond to the respective differences between the ideal modulation signals and the output of the adaptive equalizer **170**. The two-dimensional error signal E_x, E_y is provided to the weight update mechanism **101**.

The weight update mechanism **101** performs statistical analysis on accumulated samples of the error signal E_x and E_y to generate updated equalizer weights. In particular, the weight update mechanism **101** generates weights corresponding to variance of the baseband signal in a particular frequency band. The calculation of appropriate update weights or coefficients based on received error signals is well known, and may be carried out by commercially available chip sets. For example, the VCM3352 chip set available from Broadcom is capable of providing such adaptive equalizer update information.

The processor **100** also receives the tap weight coefficients or tap weights from the update mechanism **101**. The tap weight coefficients, as they exist once the equalizer **170** acquires lock, represent the inverse of the response of the channel in the time domain. The processor **100** transforms the tap weights into a relative frequency response for the channel by performing an FFT. The processor **100** then adds the relative frequency response data to the absolute signal strength result based on the raw signal strength information in order to generate the absolute level frequency response.

The processor **100** then causes the tuner **140** to tune to a new channel and repeat the process. The result is an absolute level frequency response for multiple channels. The frequency response a larger portion of the broadband signal spectrum may then be provided as a sequential stream of the individual responses of the multiple channels, as shown using four channels in **FIG. 4**. To accommodate the gap between adjacent channels, the frequency response between each channel may be interpolated.

FIG. 5, illustrates a signal constellation for a representative modulation scheme that uses a 64 point QAM. A signal constellation is a graphical representation of the possible symbols for a given modulation scheme. The horizontal and vertical axes correspond to the orthogonal components I and Q of the modulation signal. Each possible signal is represented by a point at the position of its associated (I,Q) coordinates. As shown in **FIG. 5**, 64 point QAM is represented as an array of 64 points. Since $\log_2 (64) = 6$, the choice of one particular symbol for transmission during a given symbol period can be identified using 6 bits of information. Accordingly, the coefficient produced, for example, by the I/Q decoder **180** can be identified as a relative value by reference to its QAM coordinates. The modulation control **166** (not shown) can also be based on QAM coordinates for simplifying the relative frequency response measurement.

A method of performing a sweep test of the communication system is illustrated by reference to **FIG. 6**. In the headend, the channel plan is created at step **200** and includes, among other things, information identifying the channel frequencies to be tuned to during the sweep. The channel plan may be communicated to the field unit via a variety of methods, including through transmission of telemetry information over an empty channel.

In either the headend or a field unit, a first channel under test is then selected by initializing the tuning to the digital channel at step **201**. At that point, two separate operations take place. First, the absolute system response is determined using the raw signal strength information measurement, obtained from tuner **140**, at step **202**. Second, the relative response for each channel is measured in steps **206** and **207**.

After step **202**, step **203** is performed. At step **203**, the attenuator parameters are adjusted and recorded before or while the equalizer **206** acquires lock in step **206**. It is noted that the steps **202**, **203**, **204**, **206**, and **207** can each be repeated as necessary in an iterative process, so that the single blocks shown in **FIG. 6** can each represent a number

of cycles or iterations rather than merely single steps. In addition, groups of two or more steps can be performed as nested loops (not shown).

In step **206**, the system acquires lock and then maintains a dwell time on a particular channel long enough to demodulate the channel's signal. In general, demodulators provide an interrupt or other signal notification to indicate when lock is acquired. After lock is acquired, step **207** is performed. In step **207**, an FFT is performed on the adaptive equalizer coefficients. The resultant values constitute the relative frequency response data.

After steps **203** and **207** are completed, step **204** is performed. In step **204**, the relative frequency response data is added to the absolute signal strength information result. Thereafter, in step **205**, the resultant communication system frequency response is stored and displayed for each channel. The display can be normalized for a scale common to all channels or can be set to display a relative indication compared to, e.g., a historical average.

After step **205**, step **208** is performed. In step **208**, the processor determines whether the channel under test is the last channel to be tested. If not, then the next channel is selected at step **209**. It is noted that the next channel can be tuned while the computations of step **204** and possibly **207** are being made, or while a previous value is being displayed in step **205**. If, however, it is determined at step **208** that the last channel to be tested has been tested, then step **210** is performed.

In step **210**, an extrapolation is performed between the maximum value of a given channel and the minimum value of a corresponding next adjacent channel. A straight line approximation is typically used for the extrapolation. The result of the extrapolation can either subsequently be displayed or stored at step **211**, or can be displayed or stored during the sweep. Finally, the method is repeated by returning to step **201** and causing the tuner **140** to tune to the first digital channel of the channel plan.

It will be noted that the extrapolation step **210** need not be executed only after the last channel has been measured. Likewise, the display and/or storage of the results in step **205** need not take place as each channel is measured. Indeed, all of the storage and/or display may simply take place in step **211**, thereby eliminating step **205**. Those of ordinary skill in the art may readily determine the order of those steps that best fits their implementation needs.

Although a preferred method is described using the flowchart of **FIG. 6**, in accordance with the present invention, any variation that utilizes a processor to determine the absolute signal level based on the raw signal strength information, and performs an FFT on the adaptive equalizer coefficients to generate relative frequency response information, to then combine the relative frequency response information with the absolute signal strength information, is envisaged. By repeatedly combining the relative and absolute information to generate system frequency response in an iterative process, a high level of accuracy can be achieved in a sweep test of a communication system without the need for an intrusive method.

The head end test unit sweeps the communication system by either generating and transmitting test signals at the digital channel frequencies or, if a television signal is being transmitted on a channel, using the television signal as the test signal. The remote test unit receives the information transmitted by the head end test unit and preferably sweeps the same frequencies simultaneously with the head end test unit.

Optionally, depending upon a particular implementation, additional steps may include a headend transmitting information to a field unit, a receiver transmitting information to a headend, and either the headend or the field unit subtracting the corresponding measurements of the two units to obtain a system frequency response. The transmitted information may include any partial or complete channel data, the raw signal strength information measurements' data, and/or timing information. As discussed above, the method described herein may be combined with non-intrusive methods of

performing sweep measurements on analog CATV channels to obtain an overall system response in a system that employs both digital and analog signals.